

Low EMI, Ultra-Low Distortion, 2.5-W Mono Filterless Class-D Audio Power Amplifier

DESCRIPTION

The EUA2011A is a high efficiency, 2.5W mono class-D audio power amplifier. A new developed filterless PWM modulation architecture further reduces EMI and THD+N, as well as eliminates the LC output filter, reducing external component count, system cost, and simplifying design.

Operating in a single 5V supply, EUA2011A is capable of driving 4Ω speaker load at a continuous average output of 2.5W/10% THD+N or 2W/1% THD+N. The EUA2011A has high efficiency with speaker load compared to a typical class AB amplifier. With a 3.6V supply driving an 8Ω speaker, the efficiency for a 400mW power level is 84%.

In cellular handsets, the earpiece, speaker phone, and melody ringer can each be driven by the EUA2011A. The gain of EUA2011A is externally configurable which allows independent gain control from multiple sources by summing signals from separate sources.

The EUA2011A is available in space-saving WCSP package.

FEATURES

- Unique Modulation Scheme Reduces EMI Emissions
- Efficiency at 3.6V With an 8-Ω Speaker:
 - 84% at 400 mW
- Low 2.4-mA Quiescent Current and 0.5-μA Shutdown Current
- 2.5V to 5.5V Wide Supply Voltage
- Ultra-Low Distortion - 0.07% THD+N at 1W and 8-Ω Load
- Shutdown Pin Compatible with 1.8V Logic GPIO
- Improved PSRR (-72 dB) Eliminates Need for a Voltage Regulator
- Fully Differential Design Reduces RF Rectification and Eliminates Bypass Capacitor
- Improved CMRR Eliminates Two Input Coupling Capacitors
- Internally Generated 250-kHz Switching Frequency
- Integrated Pop and Click Suppression Circuitry
- 1.5mm × 1.5mm Wafer Chip Scale Package (WCSP)
- RoHS compliant and 100% lead(Pb)-free

APPLICATIONS

- Ideal for Wireless or cellular Handsets and PDAs

Typical Application Circuit

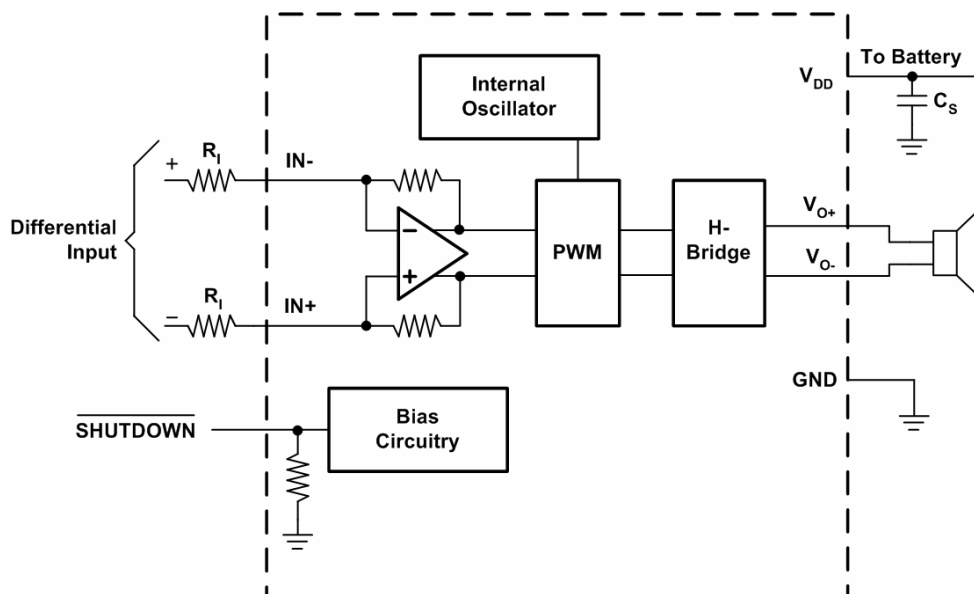


Figure1

Pin Configurations

Package Type	Pin Configurations
WCSP-9	<p style="text-align: center;">TOP VIEW</p>

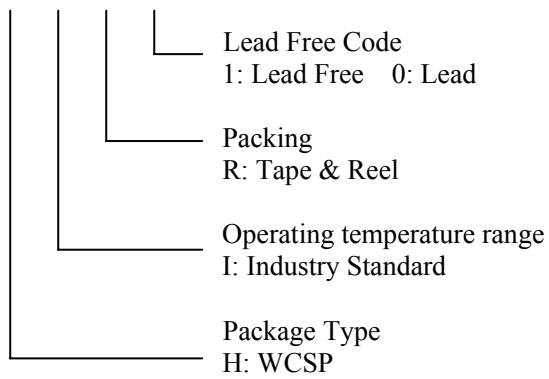
Pin Description

PIN	WCSP-9	I/O	DESCRIPTION
$\overline{\text{SHUTDOWN}}$	C2	I	Shutdown terminal (active low logic)
PV_{DD}	B2	I	Power Supply
+IN	A1	I	Positive differential input
-IN	C1	I	Negative differential input
$\text{V}_{\text{O-}}$	A3	O	Negative BTL output
V_{DD}	B1	I	Power supply
GND	A2/B3	I	High-current ground
$\text{V}_{\text{O+}}$	C3	O	Positive BTL output
NC	-		No internal connection

Ordering Information

Order Number	Package Type	Marking	Operating Temperature Range
EUA2011AHIR1	WCSP-9	xxx 70	-40 °C to 85°C

EUA2011A



Absolute Maximum Ratings

Supply Voltage, V_{DD}	-----	-0.3 V to 6V
Voltage at Any Input Pin	-----	-0.3 V to $V_{DD}+0.3V$
Junction Temperature, T_{JMAX}	-----	150°C
Storage Temperature Rang, T_{stg}	-----	-65°C to 150°C
ESD Susceptibility	-----	2kV
Lead temperature 1,6 mm (1/16 inch) from case for 10 seconds	-----	260°C
Thermal Resistance		
θ_{JA} (WCSP)	-----	77.5°C/W

Recommended Operating Conditions

	Min	Max	Unit
Supply voltage, V_{DD}	2.5	5.5	V
High-level input voltage, V_{IH}	SHUTDOWN	V_{DD}	V
Low-level input voltage, V_{IL}	SHUTDOWN	0.35	V
Input resistor, R_I	Gain $\leq 20V/V$ (26dB)	15	k
Common mode input voltage range, V_{IC}	$V_{DD}=2.5V, 5.5V, CMRR \leq -49dB$	0.5	$V_{DD}-0.8$
Operating free-air temperature, T_A	-40	85	°C

Electrical Characteristics $T_A = 25^\circ C$ (Unless otherwise noted)

Symbol	Parameter	Conditions	EUA2011A			Unit
			Min	Typ	Max.	
$ V_{OS} $	Output offset voltage (measured differentially)	$V_I=0V, A_V=2 V/V, V_{DD}=2.5V$ to 5.5V		1	25	mV
PSRR	Power supply rejection ratio	$V_{DD}= 2.5V$ to 5.5V		-72	-55	dB
CMRR	Common mode rejection ratio	$V_{DD}= 2.5V$ to 5.5V, $V_{IC}= V_{DD}/2$ to 0.5V, $V_{IC}= V_{DD}/2$ to $V_{DD}-0.8 V$		-60	-48	dB
$ I_{IH} $	High-level input current	$V_{DD}= 5.5V, V_I= 5.8V$			100	μA
$ I_{IL} $	Low-level input current	$V_{DD}= 5.5V, V_I= -0.3V$			5	μA
$I_{(Q)}$	Quiescent current	$V_{DD}= 5.5V, \text{no load}$		3.50		mA
		$V_{DD}= 3.6V, \text{no load}$		2.40		
		$V_{DD}= 2.5V, \text{no load}$		2		
$I_{(SD)}$	Shutdown current	$V(\text{SHUTDOWN})=0.35V, V_{DD}= 2.5V$ to 5.5V		0.50		μA
$r_{DS(on)}$	Static drain-source on-state resistance	$V_{DD}= 2.5V$		700		m Ω
		$V_{DD}= 3.6V$		550		
		$V_{DD}= 5.5V$		450		
	Output impedance in SHUTDOWN	$V(\text{SHUTDOWN})=0.4V$		>1		k Ω
$f_{(sw)}$	Switching frequency	$V_{DD}= 2.5V$ to 5.5V	200	250	300	kHz
	Gain	$V_{DD}= 2.5V$ to 5.5V	$\frac{280 k\Omega}{R_I}$	$\frac{300 k\Omega}{R_I}$	$\frac{320 k\Omega}{R_I}$	$\frac{V}{V}$
	Resistance from shutdown to GND			300		k Ω

Electrical Characteristics $T_A = 25^\circ\text{C}$, Gain= 2V/V, $R_L=8\Omega$ (Unless otherwise noted)

Symbol	Parameter	Conditions	EUA2011A			Unit	
			Min	Typ	Max.		
P_O	Output power	THD+N=10%, f=1kHz, $R_L=4\Omega$	$V_{DD}=5V$	2.50		W	
			$V_{DD}=3.6V$	1.25			
			$V_{DD}=2.5V$	0.58			
		THD+N=1%, f=1kHz, $R_L=4\Omega$	$V_{DD}=5V$	2		W	
			$V_{DD}=3.6V$	1			
			$V_{DD}=2.5V$	0.45			
		THD+N=10%, f=1kHz, $R_L=8\Omega$	$V_{DD}=5V$	1.58		W	
			$V_{DD}=3.6V$	0.80			
			$V_{DD}=2.5V$	0.36			
		THD+N=1%, f=1kHz, $R_L=8\Omega$	$V_{DD}=5V$	1.26		W	
			$V_{DD}=3.6V$	0.63			
			$V_{DD}=2.5V$	0.29			
THD+N	Total harmonic distortion plus noise	$V_{DD}=5V, P_O=1W, R_L=8\Omega, f=1kHz$		0.07		%	
		$V_{DD}=3.6V, P_O=0.5W, R_L=8\Omega, f=1kHz$		0.05			
		$V_{DD}=2.5V, P_O=200mW, R_L=8\Omega, f=1kHz$		0.05			
kSVR	Supply ripple rejection ratio	$V_{DD}=3.6V$, Inputs ac-grounded with $C_I=2\mu F$	f=217 Hz, $V_{(RIPPLE)}=200mV_{pp}$		-60		dB
SNR	Signal-to-noise ratio	$V_{DD}=5V, P_O=1W, R_L=8\Omega$			85		dB
V_n	Output voltage noise	$V_{DD}=3.6V$, f=20Hz to 20kHz, Inputs ac-grounded with $C_I=2\mu F$	No weighting		220		μV_{RMS}
			A weighting		96		
CMRR	Common mode rejection ratio	$V_{DD}=3.6V$, $V_{IC}=1V_{PP}$	f=217 Hz		-55		dB
Z_I	Start-up time from shutdown	$V_{DD}=3.6V$			11.5		ms

Typical Operating Characteristics

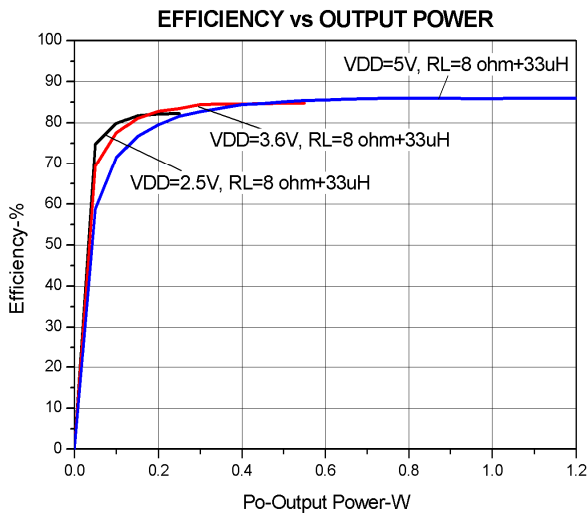


Figure2.

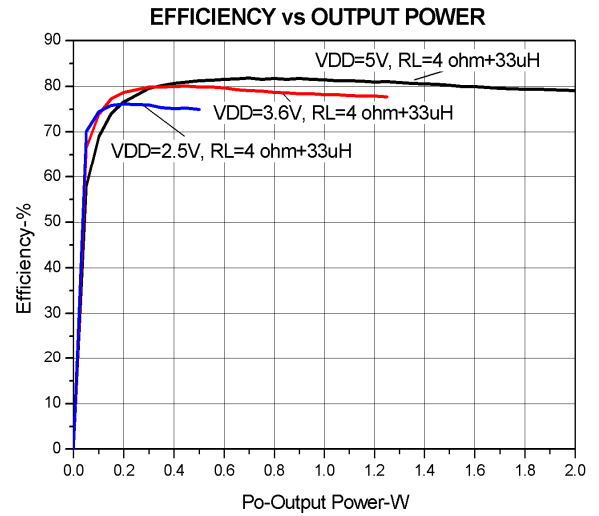


Figure3.

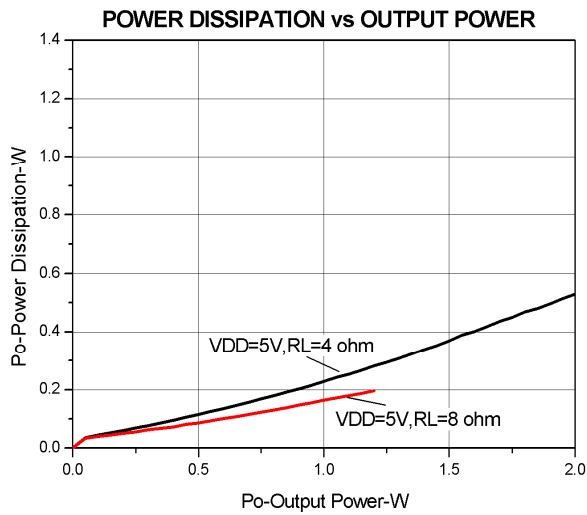


Figure4.

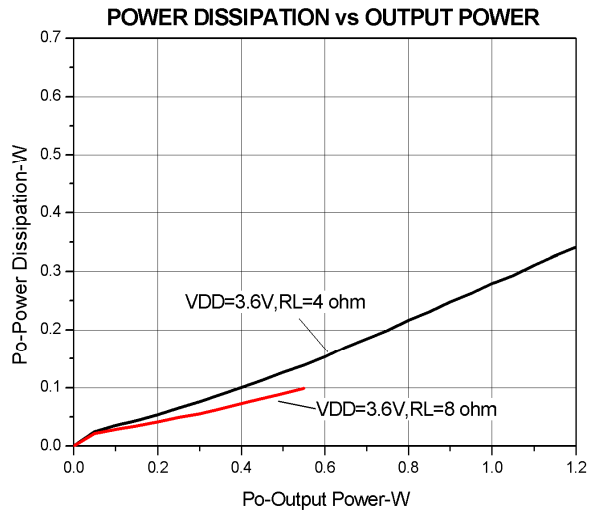


Figure5.

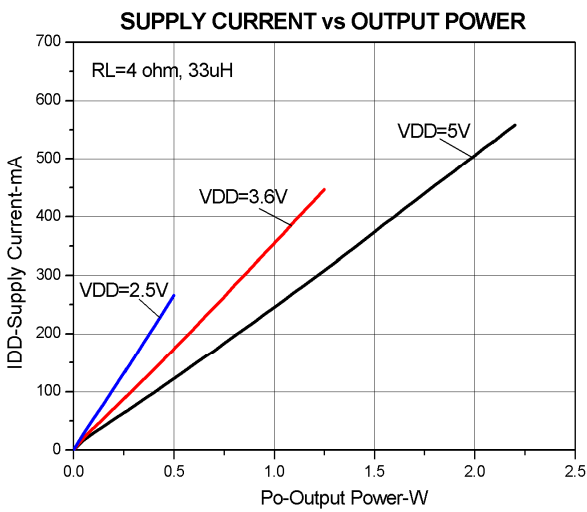


Figure6.

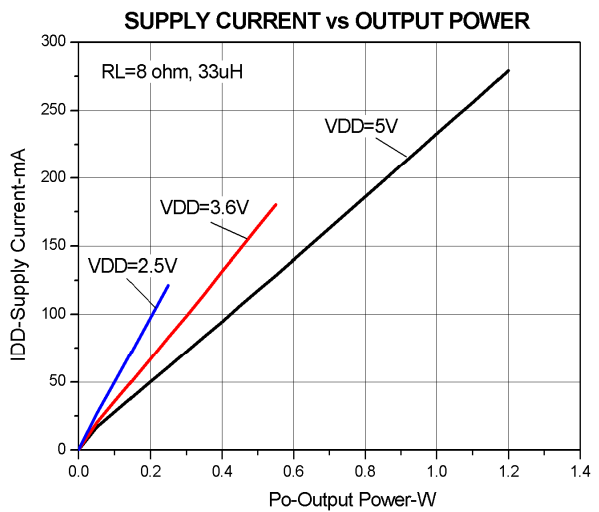


Figure7.

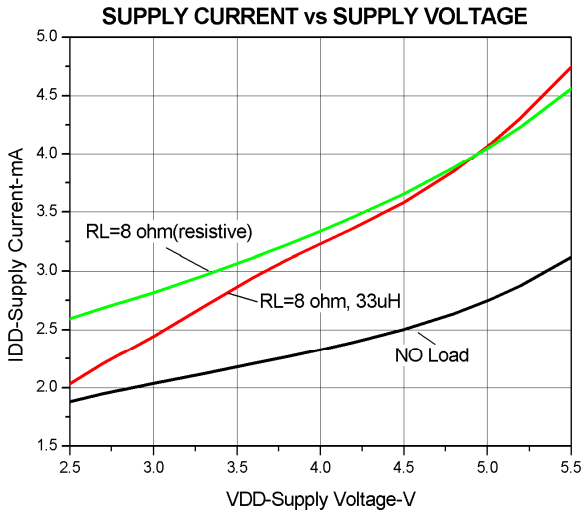


Figure8.

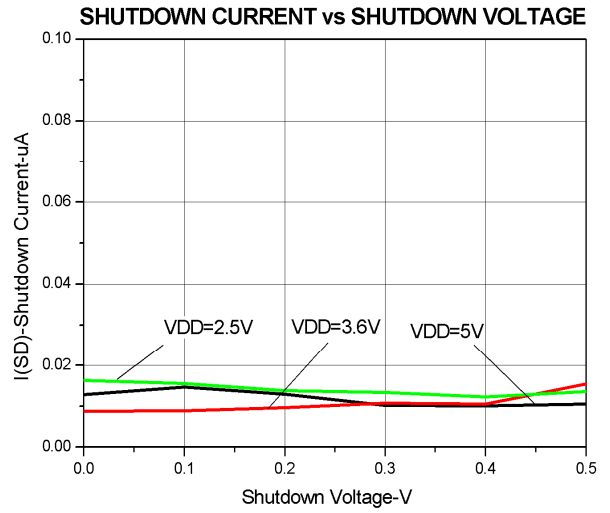


Figure9.

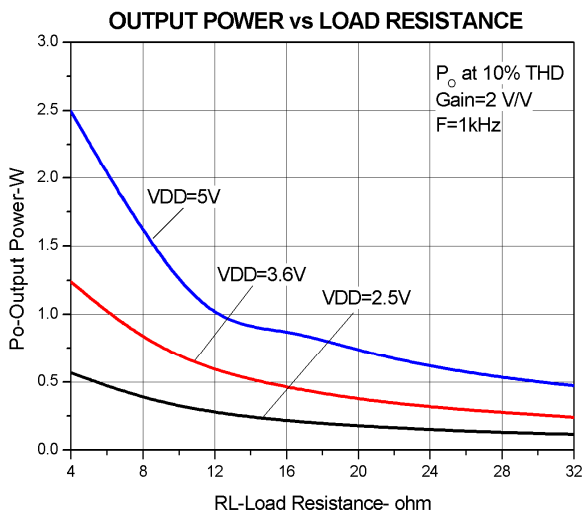


Figure10.

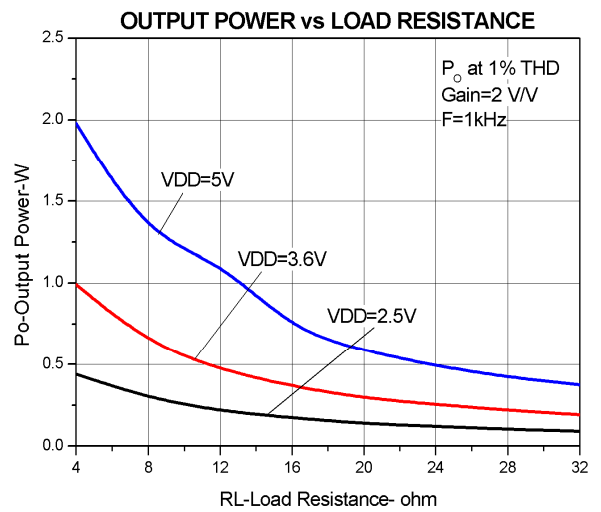


Figure11.

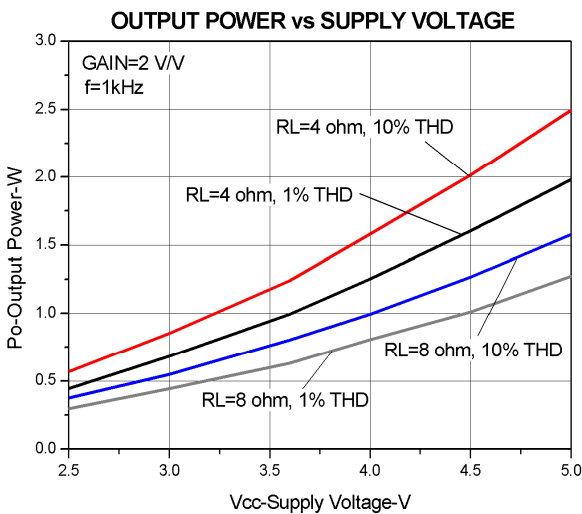


Figure12.

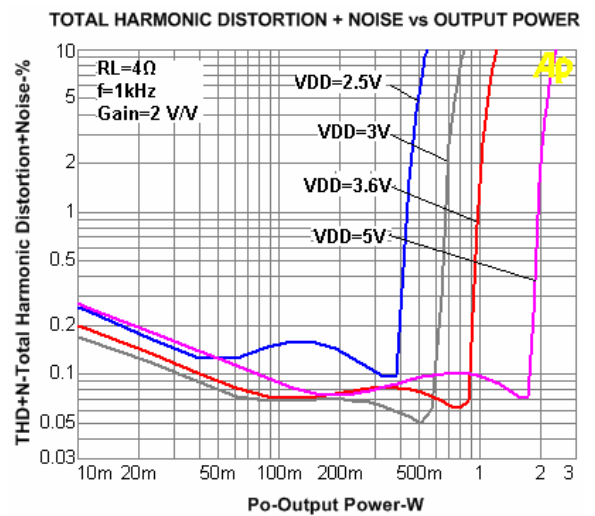


Figure13.

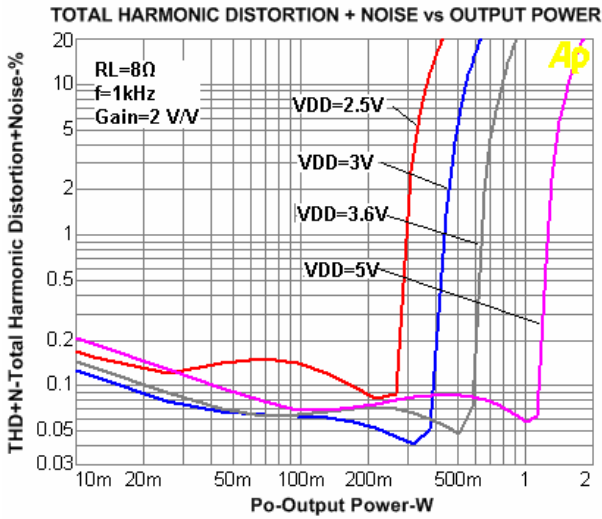


Figure14.

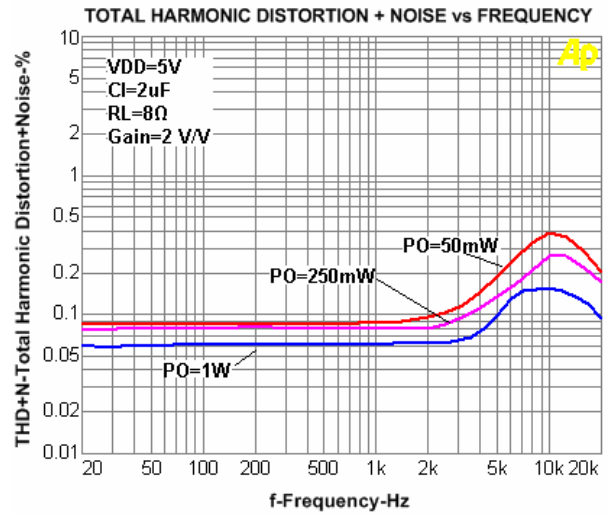


Figure15.

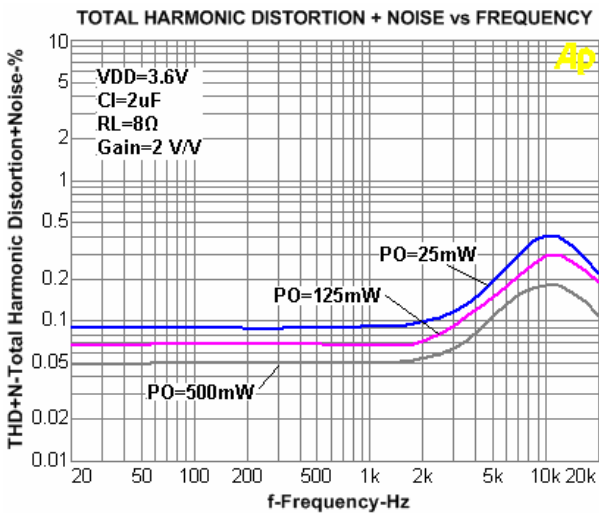


Figure16.

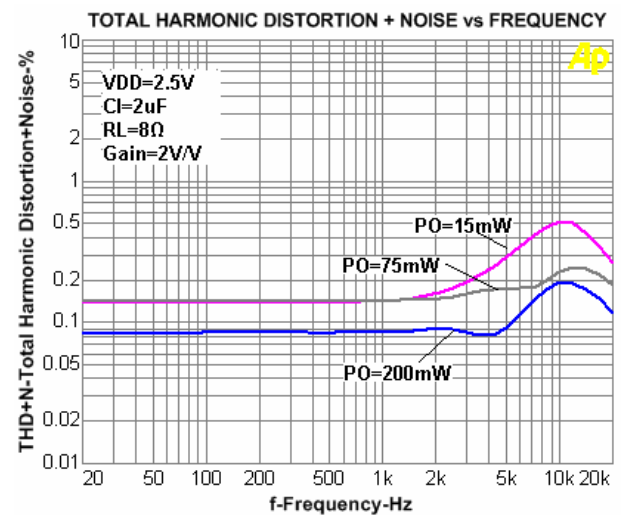


Figure17.

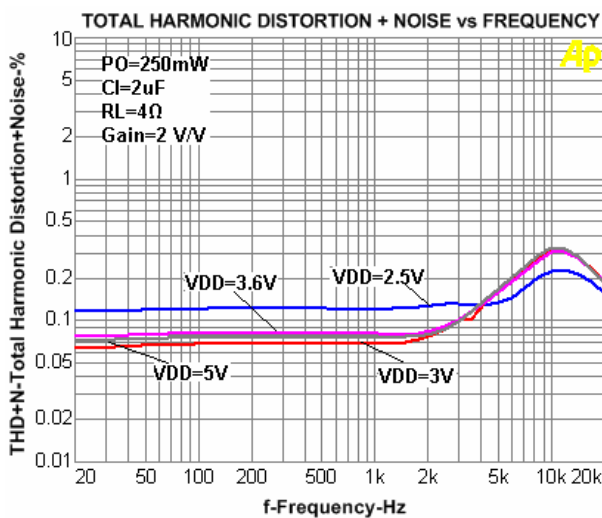


Figure18.

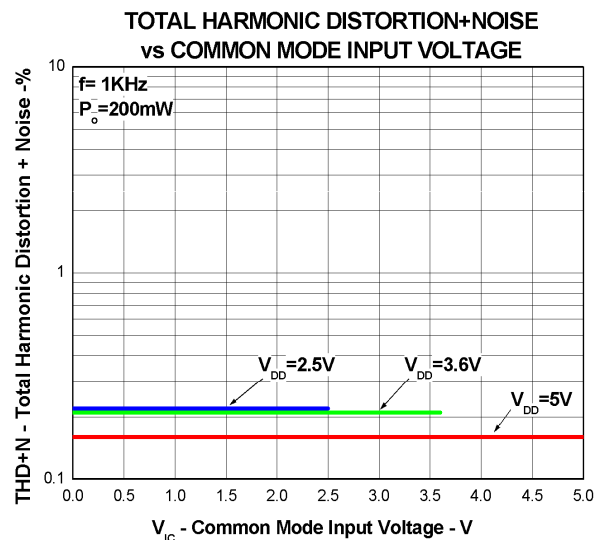


Figure19.

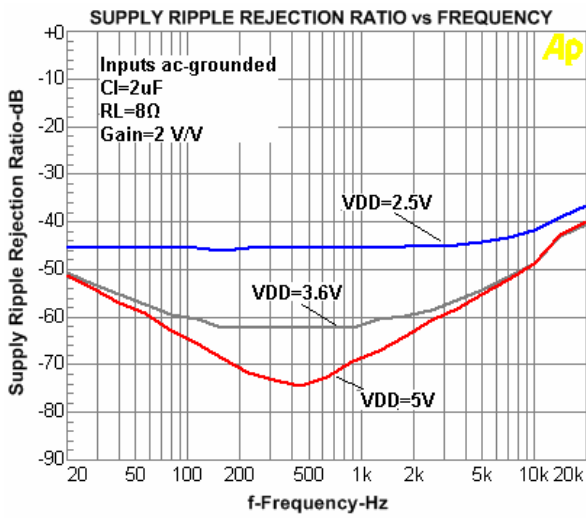


Figure20.

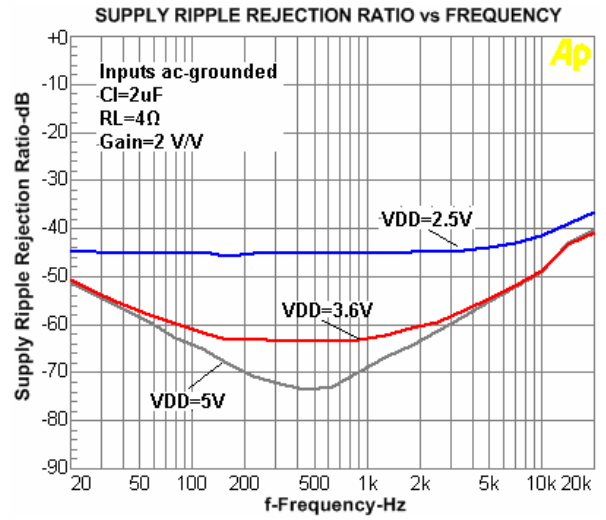


Figure21.

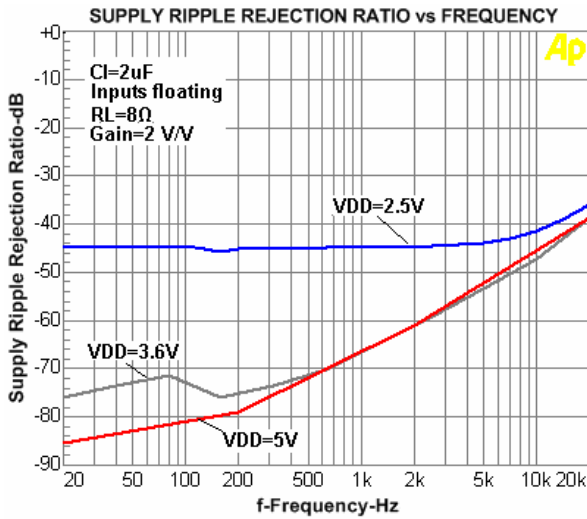


Figure22.

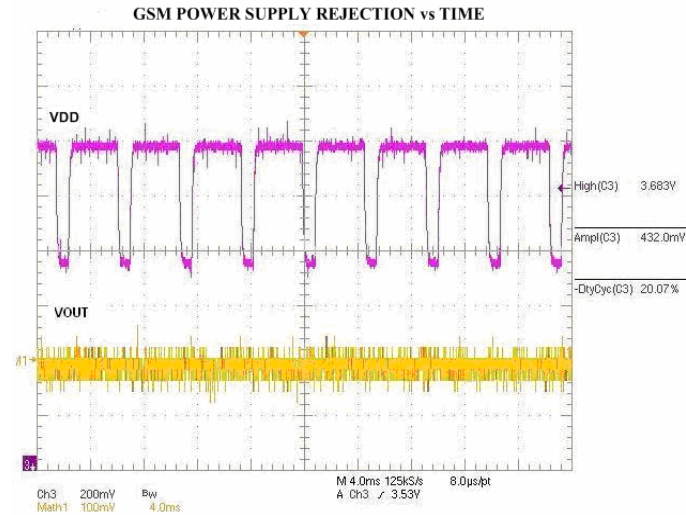


Figure23.

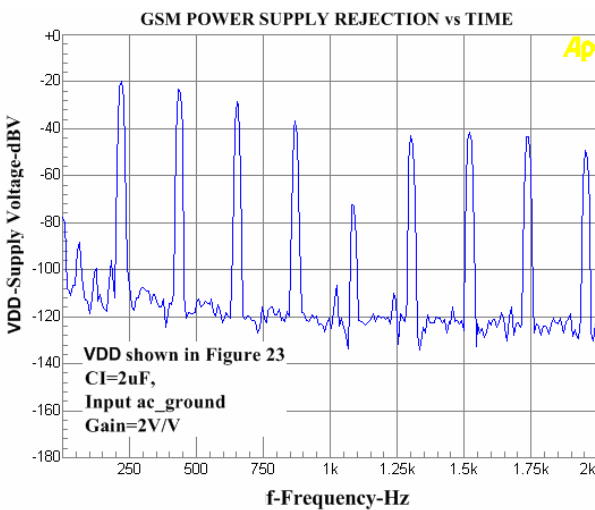


Figure24.

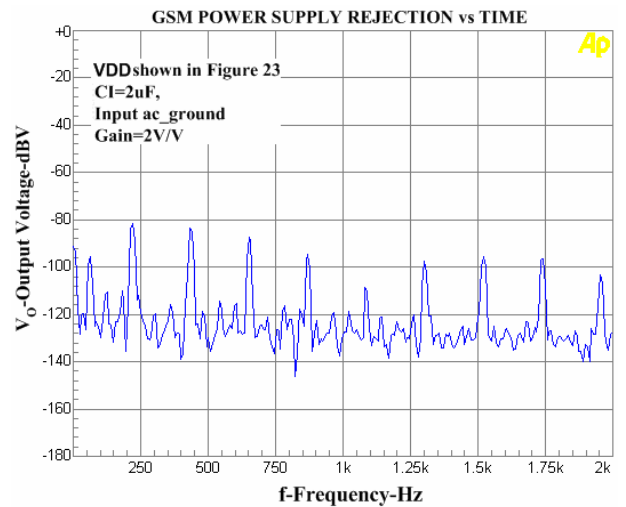


Figure25.

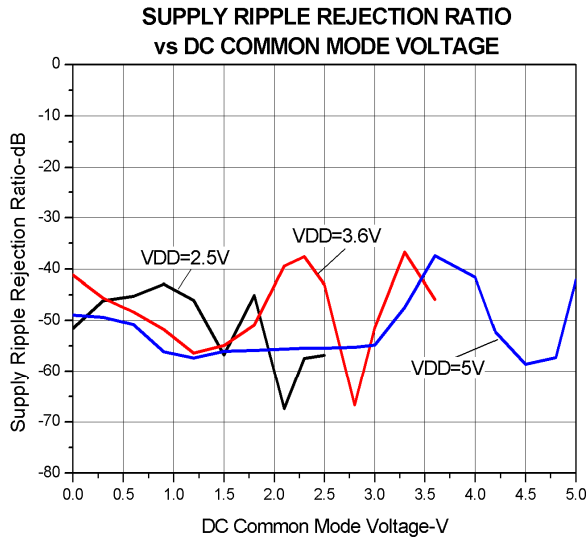


Figure26.

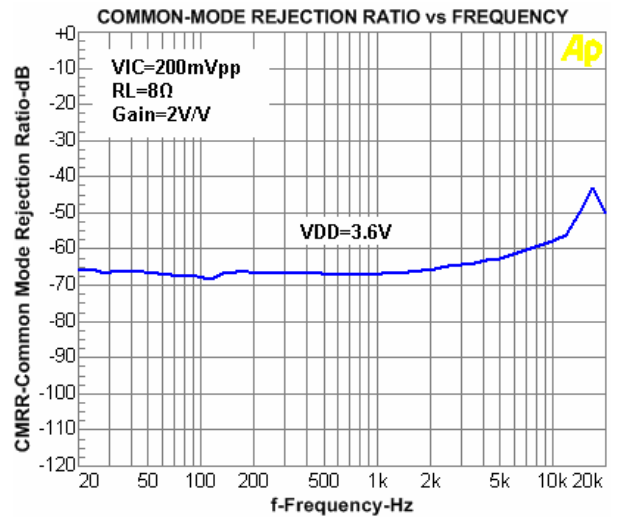


Figure27.

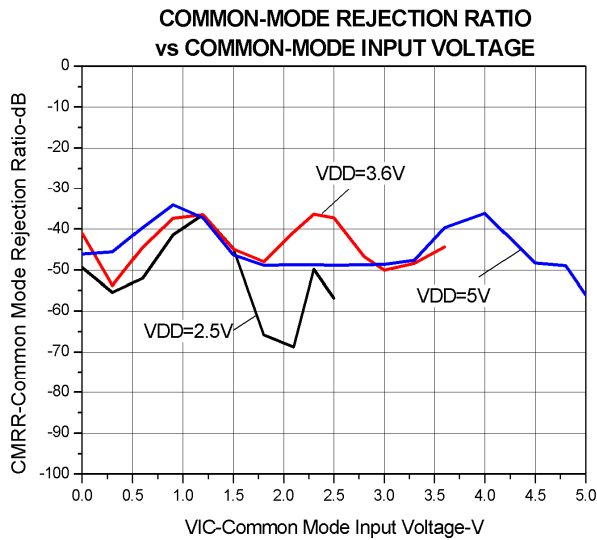


Figure28.

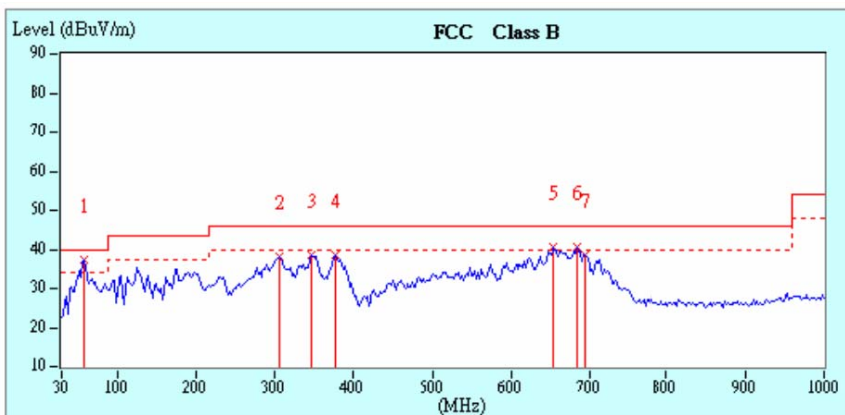


Figure29. EMI Test and FCC Limits

Application Information

Fully Differential Amplifier

The EUA2011A is a fully differential amplifier that features differential inputs and outputs. The EUA2011A also includes a common mode feedback loop that controls the output bias value to average it at $V_{CC}/2$ for any DC common mode input voltage. This allows the device to always have a maximum output voltage swing, and by consequence, maximize the output power. Moreover, as the load is connected differentially, compared to a single-ended topology, the output is four times higher for the same power supply voltage. The fully differential EUA2011A can still be used with a single-ended input; however, the EUA2011A should be used with differential inputs when in a noisy environment, like a wireless handset, to ensure maximum noise rejection.

Advantages of Fully Differential Amplifiers

The advantages of a full-differential amplifier are:

- Very high PSRR (Power Supply Rejection Ratio).
- High common mode noise rejection.
- Virtually zero pop without additional circuitry, giving an faster start-up time compared to conventional single-ended input amplifiers.
- No input coupling capacitors required thanks to common mode feedback loop.
- Midsupply bypass capacitor not required.

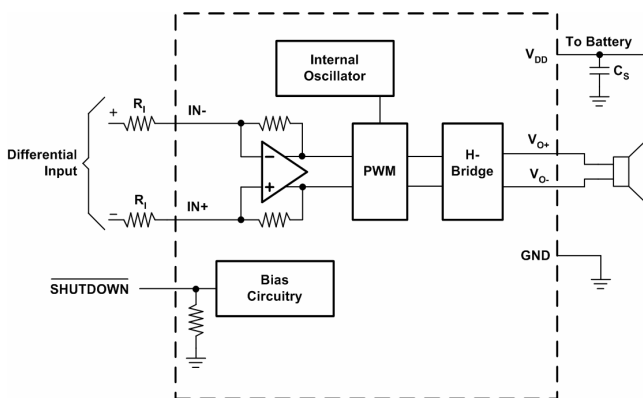


Figure 30. Differential Input Configuration

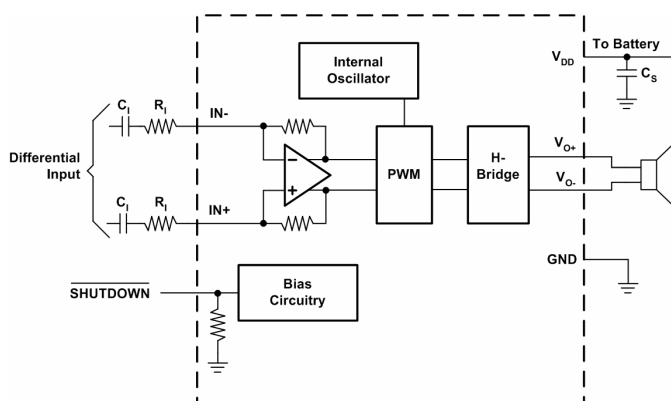


Figure 31. Differential Input Configuration and Input Capacitors

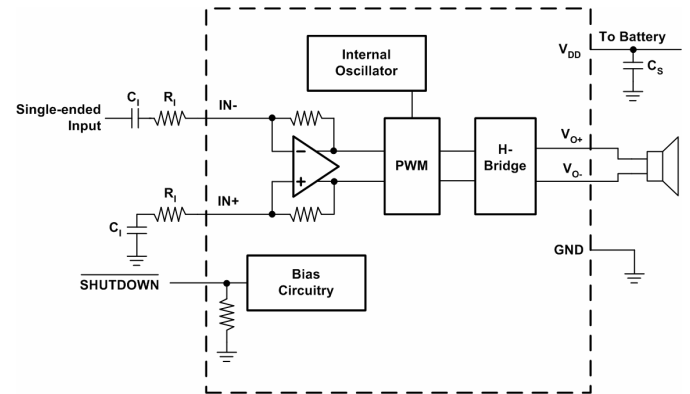


Figure 32. Single-Ended Input Configuration

Gain Selection

The input resistors (R_I) set the gain of the amplifier according to equation (1).

$$\text{Gain} = \frac{2 \times 150\text{k}\Omega}{R_I} \left(\frac{V}{V} \right) \text{-----(1)}$$

Resistor matching is very important for CMRR, PSRR, and harmonic distortion. It is recommended to use 1% tolerance resistors or better to keep the performance optimized. Matching is more important than overall tolerance. Resistor arrays with 1% matching can be used with a tolerance greater than 1%.

Keeping the input trace as short as possible to limit noise injection on the high-impedance nodes.

For optimal performance the gain should be set to 2 V/V or lower. Lower gain allows the EUA2011A to operate at its best, and keeps a high voltage at the input making the inputs less susceptible to noise.

Power Supply Decoupling Capacitor (C_s)

The EUA2011A is a high-performance CMOS class-D audio amplifier that requires adequate power supply decoupling to ensure the efficiency is high and total harmonic distortion (THD) is low. For higher frequency transients, spikes, or digital hash on the line, a good low equivalent-series-resistance (ESR) ceramic capacitor, typically $1\mu\text{F}$, placed as close as possible to the device V_{DD} lead works best. Placing this decoupling capacitor close to the EUA2011A is very important for the efficiency of the class-D amplifier, because any resistance or inductance in the trace between the device and the capacitor can cause a loss in efficiency. For filtering lower-frequency noise signals, a $10\mu\text{F}$ or greater capacitor placed near the audio power amplifier would also help.

Input Capacitors (C_I)

The EUA2011A does not require input coupling capacitors if the input signal is biased from 0.5V to V_{DD} – 0.8V. Input capacitors are required if the input signal is not biased within the recommended common-mode input range, if a high pass filtering is needed (shown in Figure 31), or if using a single-ended source (shown in Figure 32).

The input capacitors and input resistors form a high-pass filter with the corner frequency, f_c, determined in equation (2).

$$f_c = \frac{1}{(2\pi R_I C_I)} \text{-----(2)}$$

The value of the input capacitor is important to consider as it directly affects the bass (low frequency) performance of the circuit. Speakers in wireless phones cannot usually respond well to low frequencies, so the corner frequency can be set to block low frequencies in this application.

Equation (3) is reconfigured to solve for the input coupling capacitance.

$$C_I = \frac{1}{(2\pi R_I f_c)} \text{-----(3)}$$

If the corner frequency is within the audio band, the capacitors should have a tolerance of ±10% or better, because any mismatch in capacitance causes an impedance mismatch at the corner frequency and below.

Single-Ended Input Depop Function

In single-ended input application, there is an inherently voltage difference in input pairs when shutdown is released. In order to eliminate pop noise, the pop cancellation circuit need to charge the input capacitor C_I until fully-differential inputs are balanced and output power to load gradually.

The RC time constant should within the de-pop delay, if 150kΩ R_I is chosen, the recommended C_I should small than 10nF for a good pop immunity.

Summing Input Signals

The EUA2011A can be used to amplify more than one audio source. Figure 33 shows a dual differential input configuration. The gain for each input can be independently set for maximum design flexibility using the R_I resistors for each input and Equation (1). Input capacitors can be used with one or more sources as well to have different frequency responses depending on the source or if a DC voltage needs to be blocked from a source.

When using more than one single-ended source as shown in Figure 34, the impedance seen from each input terminal should be equal. To find the correct values for C_P and R_P connected to the IN+ input pin the equivalent impedance of all the single-ended sources are calculated. Equations

(4) and (5) below are for any number of single-ended sources.

$$C_P = C_{i1} + C_{i2} \text{ (F) -----(4)}$$

$$R_P = 1 / (1 / R_{i1} + 1 / R_{i2}) \text{ (}\Omega\text{) -----(5)}$$

The EUA2011A may also use a combination of single-ended and differential sources. A typical application with one single-ended source and one differential source is shown in Figure 35.

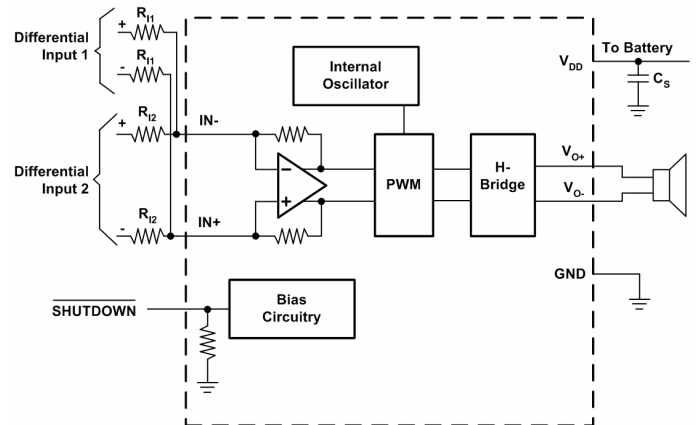


Figure 33. Dual Differential Input Configuration

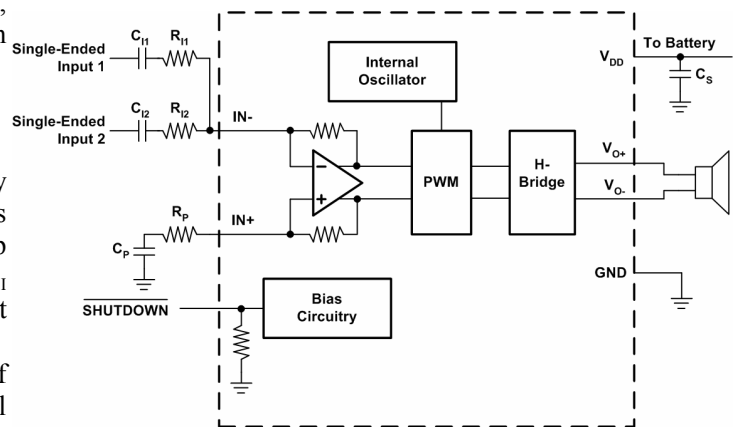


Figure 34. Dual Single-Ended Input Configuration

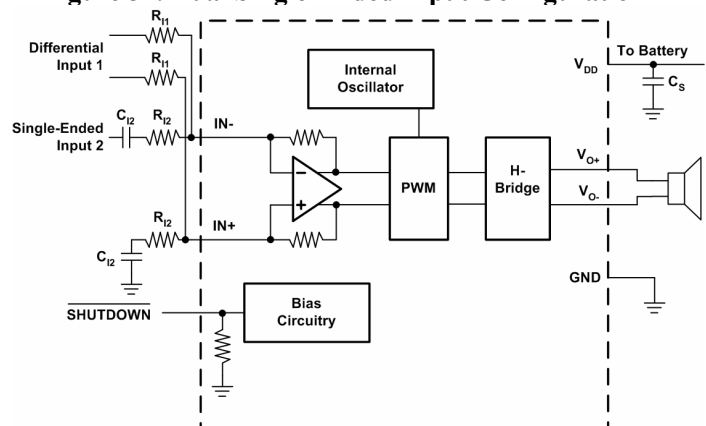


Figure 35. Dual Input with a Differential Input and Single-Ended Input

PCB Layout

As output power increases, interconnect resistance (PCB traces and wires) between the amplifier, load and power supply create a voltage drop. The voltage loss on the traces between the EUA2011A and the load results in lower output power and decreased efficiency. Higher trace resistance between the supply and the EUA2011A has the same effect as a poorly regulated supply, increase ripple on the supply line also reducing the peak output power. The effects of residual trace resistance increases as output current increases due to higher output power, decreased load impedance or both. To maintain the highest output voltage swing and corresponding peak output power, the PCB traces that connect the output pins to the load and the supply pins to the power supply should be as wide as possible to minimize trace resistance.

The use of power and ground planes will give the best THD+N performance. While reducing trace resistance, the use of power planes also creates parasitic capacitors that help to filter the power supply line.

The inductive nature of the transducer load can also result in overshoot on one or both edges, clamped by the parasitic diodes to GND and V_{DD} in each case. From an EMI stand- point, this is an aggressive waveform that can radiate or conduct to other components in the system and cause interference. It is essential to keep the power and output traces short and well shielded if possible. Use of ground planes, beads, and micro-strip layout techniques are all useful in preventing unwanted interference.

As the distance from the EUA2011A and the speaker increase, the amount of EMI radiation will increase since the output wires or traces acting as antenna become more efficient with length. What is acceptable EMI is highly application specific.

Ferrite bead placed close to the EUA2011A may be needed to reduce EMI radiation. Select a ferrite bead with the high impedance around 100MHz and a very low DCR value in the audio frequency range is the best choice. The MPZ1608S221A1 from TDK is a good choice.

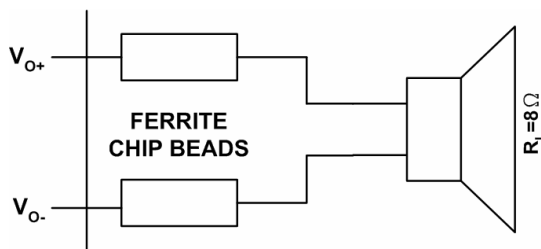
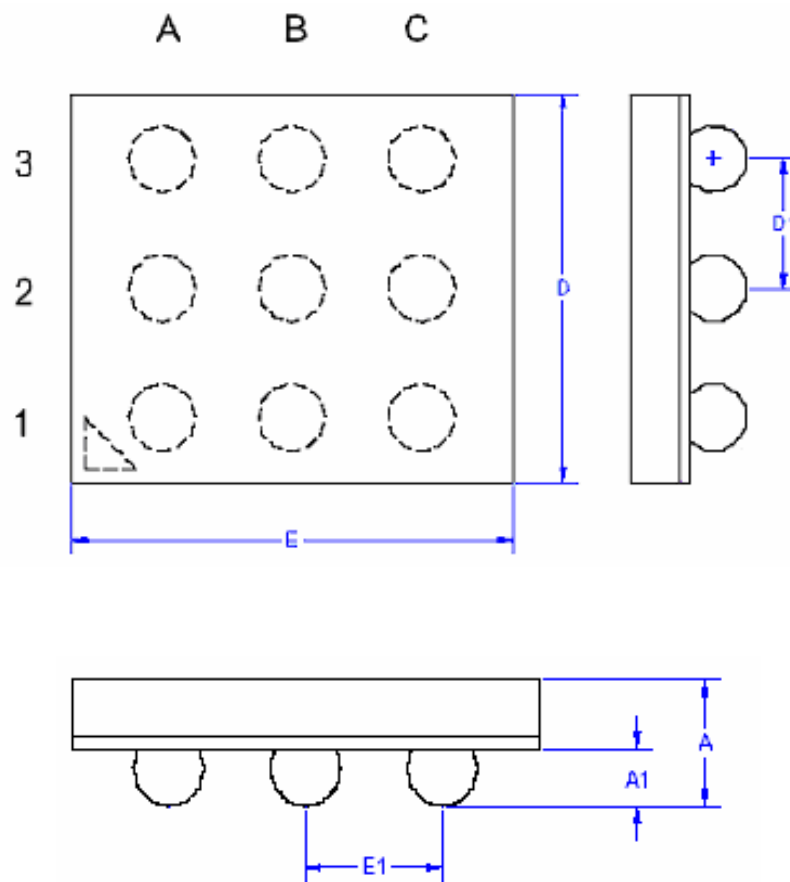


Figure 36. Optional EMI Ferrite Bead Filter

Packaging Information

WCSP-9



SYMBOLS	MILLIMETERS		INCHES	
	MIN.	MAX.	MIN.	MAX.
A	-	0.675	-	0.027
A1	0.15	0.35	0.006	0.014
D	1.45	1.55	0.057	0.061
D1	0.50		0.020	
E	1.45	1.55	0.057	0.061
E1	0.50		0.020	